Precision Low Noise, Low Input Bias Current Operational Amplifiers

OP1177/OP2177/OP4177

FEATURES
- Low offset voltage: 60 μV maximum
- Very low offset voltage drift: 0.7 μV/°C maximum
- Low input bias current: 2 nA maximum
- Low noise: 8 nV/√Hz typical
- CMRR, PSRR, and AVO > 120 dB minimum
- Low supply current: 400 μA per amplifier
- Dual supply operation: ±2.5 V to ±15 V
- Unity-gain stable
- No phase reversal
- Inputs internally protected beyond supply voltage

APPLICATIONS
- Wireless base station control circuits
- Optical network control circuits
- Instrumentation
- Sensors and controls
  - Thermocouples
  - Resistor thermal detectors (RTDs)
  - Strain bridges
- Shunt current measurements
- Precision filters

GENERAL DESCRIPTION
The OPx177 family consists of very high precision, single, dual, and quad amplifiers featuring extremely low offset voltage and drift, low input bias current, low noise, and low power consumption. Outputs are stable with capacitive loads of over 1000 pF with no external compensation. Supply current is less than 500 μA per amplifier at 30 V. Internal 500 Ω series resistors protect the inputs, allowing input signal levels several volts beyond either supply without phase reversal.

Unlike previous high voltage amplifiers with very low offset voltages, the OP1177 (single) and OP2177 (dual) amplifiers are available in tiny 8-lead surface-mount MSOP and 8-lead narrow SOIC packages. The OP4177 (quad) is available in TSSOP and 14-lead narrow SOIC packages. Moreover, specified performance in the MSOP and the TSSOP is identical to performance in the SOIC package. MSOP and TSSOP are available in tape and reel only.

The OPx177 family offers the widest specified temperature range of any high precision amplifier in surface-mount packaging. All versions are fully specified for operation from −40°C to +125°C for the most demanding operating environments.

Applications for these amplifiers include precision diode power measurement, voltage and current level setting, and level detection in optical and wireless transmission systems. Additional applications include line-powered and portable instrumentation and controls—thermocouple, RTD, strain-bridge, and other sensor signal conditioning—and precision filters.
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7/2001—Revision 0: Initial Version
### SPECIFICATIONS

#### ELECTRICAL CHARACTERISTICS

$V_S = \pm 5.0 \text{ V}, V_{CM} = 0 \text{ V}, T_A = 25^\circ \text{C}$, unless otherwise noted.

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Symbol</th>
<th>Test Conditions/Comments</th>
<th>Min</th>
<th>Typ1</th>
<th>Max</th>
<th>Unit</th>
</tr>
</thead>
<tbody>
<tr>
<td><strong>INPUT CHARACTERISTICS</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Offset Voltage</td>
<td>$V_{OS}$</td>
<td>−40°C &lt; $T_A$ &lt; +125°C</td>
<td>25</td>
<td>100</td>
<td>25</td>
<td>μV</td>
</tr>
<tr>
<td>OP2177/OP4177</td>
<td></td>
<td></td>
<td>15</td>
<td>75</td>
<td>25</td>
<td>μV</td>
</tr>
<tr>
<td>Offset Voltage</td>
<td>$V_{OS}$</td>
<td>−40°C &lt; $T_A$ &lt; +125°C</td>
<td>15</td>
<td>75</td>
<td>25</td>
<td>μV</td>
</tr>
<tr>
<td>Input Bias Current</td>
<td>$I_b$</td>
<td>−40°C &lt; $T_A$ &lt; +125°C</td>
<td>−2</td>
<td>+0.5</td>
<td>+2</td>
<td>nA</td>
</tr>
<tr>
<td>Input Offset Current</td>
<td>$I_{OS}$</td>
<td>−40°C &lt; $T_A$ &lt; +125°C</td>
<td>−1</td>
<td>+0.2</td>
<td>+1</td>
<td>nA</td>
</tr>
<tr>
<td>Input Voltage Range</td>
<td></td>
<td>−3.5 &lt; $T_A$ &lt; +3.5°C</td>
<td></td>
<td></td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>Common-Mode Rejection Ratio</td>
<td>$CMRR$</td>
<td>$V_{CM} = −3.5 \text{ V to } +3.5 \text{ V}$</td>
<td>120</td>
<td>126</td>
<td>120</td>
<td>dB</td>
</tr>
<tr>
<td>OP1177/OP2177</td>
<td></td>
<td>−40°C &lt; $T_A$ &lt; +125°C</td>
<td>118</td>
<td>125</td>
<td>118</td>
<td>dB</td>
</tr>
<tr>
<td>Large Signal Voltage Gain</td>
<td>$A_{VO}$</td>
<td>$R_L = 2 \text{ kΩ}, V_O = −3.5 \text{ V to } +3.5 \text{ V}$</td>
<td>1000</td>
<td>2000</td>
<td>1000</td>
<td>V/mV</td>
</tr>
<tr>
<td><strong>OUTPUT CHARACTERISTICS</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Output Voltage High</td>
<td>$V_{OH}$</td>
<td>$I_L = 1 \text{ mA}, −40°C &lt; T_A &lt; +125°C$</td>
<td>+4</td>
<td>+4.1</td>
<td>4</td>
<td>V</td>
</tr>
<tr>
<td>Output Voltage Low</td>
<td>$V_{OL}$</td>
<td>$I_L = 1 \text{ mA}, −40°C &lt; T_A &lt; +125°C$</td>
<td>−4.1</td>
<td>−4</td>
<td>4</td>
<td>V</td>
</tr>
<tr>
<td>Output Current</td>
<td>$I_{OUT}$</td>
<td>$V_{DROPOUT} &lt; 1.2 \text{ V}$</td>
<td>±10</td>
<td></td>
<td>10</td>
<td>mA</td>
</tr>
<tr>
<td><strong>POWER SUPPLY</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Power Supply Rejection Ratio</td>
<td>$PSRR$</td>
<td>$V_S = ±2.5 \text{ V to } ±15 \text{ V}$</td>
<td>120</td>
<td>130</td>
<td>120</td>
<td>dB</td>
</tr>
<tr>
<td>OP1177/OP4177</td>
<td></td>
<td>−40°C &lt; $T_A$ &lt; +125°C</td>
<td>115</td>
<td>125</td>
<td>115</td>
<td>dB</td>
</tr>
<tr>
<td>Supply Current per Amplifier</td>
<td>$I_{SY}$</td>
<td>$V_O = 0 \text{ V}$</td>
<td>400</td>
<td>500</td>
<td>500</td>
<td>μA</td>
</tr>
<tr>
<td><strong>DYNAMIC PERFORMANCE</strong></td>
<td></td>
<td>−40°C &lt; $T_A$ &lt; +125°C</td>
<td>114</td>
<td>120</td>
<td>114</td>
<td>dB</td>
</tr>
<tr>
<td>Slew Rate</td>
<td>$SR$</td>
<td>$R_L = 2 \text{ kΩ}$</td>
<td>0.7</td>
<td></td>
<td></td>
<td>V/μs</td>
</tr>
<tr>
<td>Gain Bandwidth Product</td>
<td>$GBP$</td>
<td></td>
<td>1.3</td>
<td></td>
<td></td>
<td>MHz</td>
</tr>
<tr>
<td><strong>NOISE PERFORMANCE</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Voltage Noise</td>
<td>$e_n$, p-p</td>
<td>0.1 Hz to 10 Hz</td>
<td>0.4</td>
<td></td>
<td></td>
<td>μV p-p</td>
</tr>
<tr>
<td>Voltage Noise Density</td>
<td>$e_n$, $f = 1 \text{ kHz}$</td>
<td>7.9</td>
<td>8.5</td>
<td>8.5</td>
<td>nV/√Hz</td>
<td></td>
</tr>
<tr>
<td>Current Noise Density</td>
<td>$I_n$, $f = 1 \text{ kHz}$</td>
<td>0.2</td>
<td></td>
<td></td>
<td>pA/√Hz</td>
<td></td>
</tr>
<tr>
<td><strong>MULTIPLE AMPLIFIERS CHANNEL SEPARATION</strong></td>
<td>$C_s$</td>
<td>$DC$</td>
<td>0.01</td>
<td></td>
<td>−120</td>
<td>μV/√Hz</td>
</tr>
<tr>
<td></td>
<td></td>
<td>$f = 100 \text{ kHz}$</td>
<td>1</td>
<td></td>
<td></td>
<td>dB</td>
</tr>
</tbody>
</table>

1 Typical values cover all parts within one standard deviation of the average value. Average values given in many competitor data sheets as typical give unrealistically low estimates for parameters that can have both positive and negative values.
ELECTRICAL CHARACTERISTICS

$V_s = \pm 15 \text{ V}, \ V_{CM} = 0 \text{ V}, \ T_A = 25^\circ \text{C}$, unless otherwise noted.

### Table 2.

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Symbol</th>
<th>Conditions</th>
<th>Min</th>
<th>Typ1</th>
<th>Max</th>
<th>Unit</th>
</tr>
</thead>
<tbody>
<tr>
<td><strong>INPUT CHARACTERISTICS</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Offset Voltage</td>
<td>$V_{OS}$</td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>25</td>
<td>100</td>
<td></td>
<td>μV</td>
</tr>
<tr>
<td>OP1177</td>
<td></td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>25</td>
<td>120</td>
<td></td>
<td>μV</td>
</tr>
<tr>
<td>OP2177/OP4177</td>
<td>$V_{OS}$</td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>25</td>
<td>100</td>
<td></td>
<td>μV</td>
</tr>
<tr>
<td>OP4177</td>
<td>$V_{OS}$</td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>25</td>
<td>120</td>
<td></td>
<td>μV</td>
</tr>
<tr>
<td>Input Bias Current</td>
<td>$I_B$</td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>-2</td>
<td>+0.5</td>
<td>+2</td>
<td>nA</td>
</tr>
<tr>
<td>Input Offset Current</td>
<td>$I_{OS}$</td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>-1</td>
<td>+0.2</td>
<td>+1</td>
<td>nA</td>
</tr>
<tr>
<td>Input Voltage Range</td>
<td></td>
<td>$-13.5 &lt; V_s &lt; +13.5 \text{ V}$</td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Common-Mode Rejection Ratio</td>
<td>CMRR</td>
<td>$V_{CM} = -13.5 \text{ V}$ to $+13.5 \text{ V}$</td>
<td>120</td>
<td>125</td>
<td></td>
<td>dB</td>
</tr>
<tr>
<td>Large Signal Voltage Gain</td>
<td>$A_{VO}$</td>
<td>$R_L = 2 \text{ kΩ}, \ V_O = -13.5 \text{ V}$</td>
<td>1000</td>
<td>3000</td>
<td></td>
<td>V/mV</td>
</tr>
<tr>
<td>Offset Voltage Drift</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>OP1177/OP2177</td>
<td>$\Delta V_{OS}/\Delta T$</td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>0.2</td>
<td>0.7</td>
<td></td>
<td>μV/^\circ \text{C}</td>
</tr>
<tr>
<td>OP4177</td>
<td>$\Delta V_{OS}/\Delta T$</td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>0.3</td>
<td>0.9</td>
<td></td>
<td>μV/^\circ \text{C}</td>
</tr>
<tr>
<td><strong>OUTPUT CHARACTERISTICS</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Output Voltage High</td>
<td>$V_{OH}$</td>
<td>$I_L = 1 \text{ mA}, \ -40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>+14</td>
<td>+14.1</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>Output Voltage Low</td>
<td>$V_{OL}$</td>
<td>$I_L = 1 \text{ mA}, \ -40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>-14</td>
<td>-14</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>Output Current</td>
<td>$I_{OUT}$</td>
<td>$V_{DROPOUT} &lt; 1.2 \text{ V}$</td>
<td>±10</td>
<td></td>
<td></td>
<td>mA</td>
</tr>
<tr>
<td>Short-Circuit Current</td>
<td>$I_{SC}$</td>
<td></td>
<td>±25</td>
<td></td>
<td></td>
<td>mA</td>
</tr>
<tr>
<td><strong>POWER SUPPLY</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Power Supply Rejection Ratio</td>
<td>PSRR</td>
<td>$V_s = \pm 2.5 \text{ V}$ to $\pm 15 \text{ V}$</td>
<td>120</td>
<td>130</td>
<td></td>
<td>dB</td>
</tr>
<tr>
<td>OP1177</td>
<td></td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>115</td>
<td>125</td>
<td></td>
<td>dB</td>
</tr>
<tr>
<td>OP2177/OP4177</td>
<td></td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>118</td>
<td>121</td>
<td></td>
<td>dB</td>
</tr>
<tr>
<td>Supply Current per Amplifier</td>
<td>$I_{SY}$</td>
<td>$V_O = 0 \text{ V}$</td>
<td>400</td>
<td>500</td>
<td></td>
<td>μA</td>
</tr>
<tr>
<td></td>
<td></td>
<td>$-40^\circ \text{C} &lt; T_A &lt; +125^\circ \text{C}$</td>
<td>114</td>
<td>120</td>
<td></td>
<td>dB</td>
</tr>
<tr>
<td><strong>DYNAMIC PERFORMANCE</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Slew Rate</td>
<td>SR</td>
<td>$R_L = 2 \text{ kΩ}$</td>
<td>0.7</td>
<td></td>
<td></td>
<td>V/μs</td>
</tr>
<tr>
<td>Gain Bandwidth Product</td>
<td>GBP</td>
<td></td>
<td>1.3</td>
<td></td>
<td></td>
<td>MHz</td>
</tr>
<tr>
<td><strong>NOISE PERFORMANCE</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Voltage Noise</td>
<td>$e_v$</td>
<td>$0.1 \text{ Hz}$ to $10 \text{ Hz}$</td>
<td>0.4</td>
<td></td>
<td></td>
<td>μV p-p</td>
</tr>
<tr>
<td>Voltage Noise Density</td>
<td>$e_v$</td>
<td>$f = 1 \text{ kHz}$</td>
<td>7.9</td>
<td>8.5</td>
<td></td>
<td>nV/√Hz</td>
</tr>
<tr>
<td>Current Noise Density</td>
<td>$i_n$</td>
<td>$f = 1 \text{ kHz}$</td>
<td>0.2</td>
<td></td>
<td></td>
<td>pA/√Hz</td>
</tr>
<tr>
<td><strong>MULTIPLE AMPLIFIERS CHANNEL SEPARATION</strong></td>
<td>$C_s$</td>
<td>DC</td>
<td>0.01</td>
<td></td>
<td></td>
<td>μV/V</td>
</tr>
<tr>
<td></td>
<td></td>
<td>$f = 100 \text{ kHz}$</td>
<td>−120</td>
<td></td>
<td></td>
<td>dB</td>
</tr>
</tbody>
</table>

1 Typical values cover all parts within one standard deviation of the average value. Average values given in many competitor data sheets as typical give unrealistically low estimates for parameters that can have both positive and negative values.
ABSOLUTE MAXIMUM RATINGS

Table 3.

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Rating</th>
</tr>
</thead>
<tbody>
<tr>
<td>Supply Voltage</td>
<td>36 V</td>
</tr>
<tr>
<td>Input Voltage</td>
<td>$V_{S-}$ to $V_{S+}$</td>
</tr>
<tr>
<td>Differential Input Voltage</td>
<td>$\pm$ Supply Voltage</td>
</tr>
<tr>
<td>Storage Temperature Range</td>
<td>−65°C to +150°C</td>
</tr>
<tr>
<td>R, RM, and RU Packages</td>
<td></td>
</tr>
<tr>
<td>Operating Temperature Range</td>
<td>−40°C to +125°C</td>
</tr>
<tr>
<td>OP1177/OP2177/OP4177</td>
<td></td>
</tr>
<tr>
<td>Junction Temperature Range</td>
<td>−65°C to +150°C</td>
</tr>
<tr>
<td>R, RM, and RU Packages</td>
<td></td>
</tr>
<tr>
<td>Lead Temperature, Soldering (10 sec)</td>
<td>300°C</td>
</tr>
</tbody>
</table>

Stresses at or above those listed under Absolute Maximum Ratings may cause permanent damage to the product. This is a stress rating only; functional operation of the product at these or any other conditions above those indicated in the operational section of this specification is not implied. Operation beyond the maximum operating conditions for extended periods may affect product reliability.

THERMAL RESISTANCE

$\theta_{JA}$ is specified for the worst-case conditions, that is, a device soldered in a circuit board for surface-mount packages.

Table 4. Thermal Resistance

<table>
<thead>
<tr>
<th>Package Type</th>
<th>$\theta_{JA}$</th>
<th>$\theta_{JC}$</th>
<th>Unit</th>
</tr>
</thead>
<tbody>
<tr>
<td>8-Lead MSOP (RM-8)</td>
<td>190</td>
<td>44</td>
<td>°C/W</td>
</tr>
<tr>
<td>8-Lead SOIC_N (R-8)</td>
<td>158</td>
<td>43</td>
<td>°C/W</td>
</tr>
<tr>
<td>14-Lead SOIC_N (R-14)</td>
<td>120</td>
<td>36</td>
<td>°C/W</td>
</tr>
<tr>
<td>14-Lead TSSOP (RU-14)</td>
<td>240</td>
<td>43</td>
<td>°C/W</td>
</tr>
</tbody>
</table>

1 MSOP is available in tape and reel only.

ESD CAUTION

**ESD (electrostatic discharge) sensitive device.** Charged devices and circuit boards can discharge without detection. Although this product features patented or proprietary protection circuitry, damage may occur on devices subjected to high energy ESD. Therefore, proper ESD precautions should be taken to avoid performance degradation or loss of functionality.
TYPICAL PERFORMANCE CHARACTERISTICS

Figure 7. Input Offset Voltage Distribution

Figure 8. Input Offset Voltage Drift Distribution

Figure 9. Input Bias Current Distribution

Figure 10. Output Voltage to Supply Rail vs. Load Current

Figure 11. Input Bias Current vs. Temperature

Figure 12. Open-Loop Gain and Phase Shift vs. Frequency
### Closed-Loop Gain vs. Frequency

<table>
<thead>
<tr>
<th>FREQUENCY (Hz)</th>
<th>10k</th>
<th>100k</th>
<th>1M</th>
<th>10M</th>
</tr>
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<tbody>
<tr>
<td>CLOSED-LOOP GAIN (dB)</td>
<td>100</td>
<td>80</td>
<td>60</td>
<td>40</td>
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</table>

### Output Impedance vs. Frequency

<table>
<thead>
<tr>
<th>FREQUENCY (Hz)</th>
<th>1k</th>
<th>10k</th>
<th>100k</th>
<th>1M</th>
</tr>
</thead>
<tbody>
<tr>
<td>OUTPUT IMPEDANCE (Ω)</td>
<td>450</td>
<td>400</td>
<td>350</td>
<td>300</td>
</tr>
</tbody>
</table>

### Small Signal Transient Response

- **Figure 15. Large Signal Transient Response**
- **Figure 16. Small Signal Transient Response**
- **Figure 17. Small Signal Overshoot vs. Load Capacitance**
- **Figure 18. Positive Overvoltage Recovery**
Figure 19. Negative Overvoltage Recovery

Figure 20. CMRR vs. Frequency

Figure 21. PSRR vs. Frequency

Figure 22. 0.1 Hz to 10 Hz Input Voltage Noise

Figure 23. Voltage Noise Density vs. Frequency

Figure 24. Short-Circuit Current vs. Temperature
Figure 25. Output Voltage Swing vs. Temperature

Figure 26. Warm-Up Drift

Figure 27. Input Offset Voltage vs. Temperature

Figure 28. CMRR vs. Temperature

Figure 29. PSRR vs. Temperature

Figure 30. Input Offset Voltage Distribution
Figure 31. Output Voltage to Supply Rail vs. Load Current

Figure 32. Open-Loop Gain and Phase Shift vs. Frequency

Figure 33. Closed-Loop Gain vs. Frequency

Figure 34. Output Impedance vs. Frequency

Figure 35. Large Signal Transient Response

Figure 36. Small Signal Transient Response
Figure 37. Small Signal Overshoot vs. Load Capacitance

Figure 38. Positive Overvoltage Recovery

Figure 39. Negative Overvoltage Recovery

Figure 40. No Phase Reversal

Figure 41. CMRR vs. Frequency

Figure 42. PSRR vs. Frequency
Figure 43. 0.1 Hz to 10 Hz Input Voltage Noise

Figure 44. Voltage Noise Density vs. Frequency

Figure 45. Short-Circuit Current vs. Temperature

Figure 46. Output Voltage Swing vs. Temperature

Figure 47. Input Offset Voltage vs. Temperature

Figure 48. Supply Current vs. Temperature
Figure 49. Supply Current vs. Supply Voltage

Figure 50. Channel Separation vs. Frequency
FUNCTIONAL DESCRIPTION

The OPx177 series is the fourth generation of Analog Devices, Inc., industry-standard OP07 amplifier family. OPx177 is a high precision, low noise operational amplifier with a combination of extremely low offset voltage and very low input bias currents. Unlike JFET amplifiers, the low bias and offset currents are relatively insensitive to ambient temperatures, even up to 125°C.

Analog Devices proprietary process technology and linear design expertise has produced a high voltage amplifier with superior performance to the OP07, OP77, and OP177 in a tiny MSOP 8-lead package. Despite its small size, the OPx177 offers numerous improvements, including low wideband noise, very wide input and output voltage range, lower input bias current, and complete freedom from phase inversion.

OPx177 has a specified operating temperature range as wide as any similar device in a plastic surface-mount package. This is increasingly important as PCB and overall system sizes continue to shrink, causing internal system temperatures to rise. Power consumption is reduced by a factor of four from the OP177, and bandwidth and slew rate increase by a factor of two. The low power dissipation and very stable performance vs. temperature also act to reduce warmup drift errors to insignificant levels.

The total equivalent rms noise over a specific bandwidth is expressed as

\[ e_n = \left( e_{n,\text{TOTAL}} \right)^{1/2} \sqrt{BW} \]

where \( BW \) is the bandwidth in hertz.

The preceding analysis is valid for frequencies larger than 50 Hz. When considering lower frequencies, flicker noise (also known as 1/f noise) must be taken into account.

For a reference on noise calculations, refer to the Band-Pass KRC or Sallen-Key Filter section.

GAIN LINEARITY

Gain linearity reduces errors in closed-loop configurations. The straighter the gain curve, the lower the maximum error over the input signal range. This is especially true for circuits with high closed-loop gains.

The OP1177 has excellent gain linearity even with heavy loads, as shown in Figure 51. Compare its performance to the OPA277, shown in Figure 52. Both devices are measured under identical conditions, with \( R_L = 2 \, \text{k}\Omega \). The OP2177 (dual) has virtually no distortion at lower voltages. Compared to the OPA277 at several supply voltages and various loads, OP1177 performance far exceeds that of its counterpart.

For \( R_S < 3.9 \, \text{k}\Omega \), \( e_n \) dominates and

\[ e_{n,\text{TOTAL}} \approx e_n \]

For \( 3.9 \, \text{k}\Omega < R_S < 412 \, \text{k}\Omega \), voltage noise of the amplifier, the current noise of the amplifier translated through the source resistor, and the thermal noise from the source resistor all contribute to the total noise.

For \( R_S > 412 \, \text{k}\Omega \), the current noise dominates and

\[ e_{n,\text{TOTAL}} \approx I_i R_S \]

The total noise density of the OPx177 is

\[ e_{n,\text{TOTAL}} = \sqrt{e_n^2 + i_i R_S^2} + 4kTR_S \]

where:
- \( e_n \) is the input voltage noise density.
- \( i_i \) is the input current noise density.
- \( R_S \) is the source resistance at the noninverting terminal.
- \( k \) is Boltzmann’s constant (\( 1.38 \times 10^{-23} \, \text{J/K} \)).
- \( T \) is the ambient temperature in Kelvin (\( T = 273 + \) temperature in degrees Celsius).
INPUT OVERVOLTAGE PROTECTION

When input voltages exceed the positive or negative supply voltage, most amplifiers require external resistors to protect them from damage. The OPx177 has internal protective circuitry that allows voltages as high as 2.5 V beyond the supplies to be applied at the input of either terminal without any harmful effects. Use an additional resistor in series with the inputs if the voltage exceeds the supplies by more than 2.5 V. The value of the resistor can be determined from the formula

\[
\frac{(V_{ov} - V_s)}{R_s + 500 \, \Omega} \leq 5 \, \text{mA}
\]

With the OPx177 low input offset current of <1 nA maximum, placing a 5 kΩ resistor in series with both inputs adds less than 5 μV to input offset voltage and has a negligible impact on the overall noise performance of the circuit.

5 kΩ protects the inputs to more than 27 V beyond either supply. Refer to the THD + Noise section for additional information on noise vs. source resistance.

OUTPUT PHASE REVERSAL

Phase reversal is defined as a change of polarity in the amplifier transfer function. Many operational amplifiers exhibit phase reversal when the voltage applied to the input is greater than the maximum common-mode voltage. In some instances, this can cause permanent damage to the amplifier. In feedback loops, it can result in system lockups or equipment damage. The OPx177 is immune to phase reversal problems even at input voltages beyond the supplies.

SETTLING TIME

Settling time is defined as the time it takes an amplifier output to reach and remain within a percentage of its final value after application of an input pulse. It is especially important in measurement and control circuits in which amplifiers buffer ADC inputs or DAC outputs.

To minimize settling time in amplifier circuits, use proper bypassing of power supplies and an appropriate choice of circuit components. Resistors should be metal film types, because they have less stray capacitance and inductance than their wire-wound counterparts. Capacitors should be polystyrene or polycarbonate types to minimize dielectric absorption.

The leads from the power supply should be kept as short as possible to minimize capacitance and inductance. The OPx177 has a settling time of about 45 μs to 0.01% (1 mV) with a 10 V step applied to the input in a noninverting unity gain.

OVERLOAD RECOVERY TIME

Overload recovery is defined as the time it takes the output voltage of an amplifier to recover from a saturated condition to its linear response region. A common example is one in which the output voltage demanded by the transfer function of the circuit lies beyond the maximum output voltage capability of the amplifier. A 10 V input applied to an amplifier in a closed-loop gain of 2 demands an output voltage of 20 V. This is beyond the output voltage range of the OPx177 when operating at ±15 V supplies and forces the output into saturation.

Recovery time is important in many applications, particularly where the operational amplifier must amplify small signals in the presence of large transient voltages.
Figure 54. Test Circuit for Overload Recovery Time

Figure 18 shows the positive overload recovery time of the OP1177. The output recovers in less than 4 μs after being overdriven by more than 100%.

The negative overload recovery of the OP1177 is 1.4 μs, as seen in Figure 19.

THD + NOISE

The OPx177 has very low total harmonic distortion. This indicates excellent gain linearity and makes the OPx177 a great choice for high closed-loop gain precision circuits.

Figure 55 shows that the OPx177 has approximately 0.00025% distortion in unity gain, the worst-case configuration for distortion.

CAPACITIVE LOAD DRIVE

OPx177 is inherently stable at all gains and capable of driving large capacitive loads without oscillation. With no external compensation, the OPx177 safely drives capacitive loads up to 1000 pF in any configuration. As with virtually any amplifier, driving larger capacitive loads in unity gain requires additional circuitry to assure stability.

In this case, a snubber network is used to prevent oscillation and reduce the amount of overshoot. A significant advantage of this method is that it does not reduce the output swing because the Resistor Rs is not inside the feedback loop.

Figure 56 is a scope shot of the output of the OPx177 in response to a 400 mV pulse. The load capacitance is 2 nF. The circuit is configured in positive unity gain, the worst-case condition for stability.

As shown in Figure 58, placing an R-C network parallel to the load capacitance (C_L) allows the amplifier to drive higher values of C_L without causing oscillation or excessive overshoot.

There is no ringing, and overshoot is reduced from 27% to 5% using the snubber network.

Optimum values for Rs and Cs are tabulated in Table 5 for several capacitive loads, up to 200 nF. Values for other capacitive loads can be determined experimentally.

Table 5. Optimum Values for Capacitive Loads

<table>
<thead>
<tr>
<th>C_L</th>
<th>Rs</th>
<th>Cs</th>
</tr>
</thead>
<tbody>
<tr>
<td>10 nF</td>
<td>20 Ω</td>
<td>0.33 μF</td>
</tr>
<tr>
<td>50 nF</td>
<td>30 Ω</td>
<td>6.8 nF</td>
</tr>
<tr>
<td>200 nF</td>
<td>200 Ω</td>
<td>0.47 μF</td>
</tr>
</tbody>
</table>
Caution: The snubber technique cannot recover the loss of bandwidth induced by large capacitive loads.

**STRAY INPUT CAPACITANCE COMPENSATION**

The effective input capacitance in an operational amplifier circuit \( C_t \) consists of three components. These are the internal differential capacitance between the input terminals, the internal common-mode capacitance of each input to ground, and the external capacitance including parasitic capacitance. In the circuit in Figure 59, the closed-loop gain increases as the signal frequency increases.

The transfer function of the circuit is

\[
1 + \frac{R_2}{R_1} (1 + sC_t R_1)
\]

indicating a zero at

\[
s = \frac{R_2 + R_1}{2\pi R_1 C_t} = \frac{1}{2\pi (R_1/R_2) C_t}
\]

Depending on the value of \( R_1 \) and \( R_2 \), the cutoff frequency of the closed-loop gain can be well below the crossover frequency. In this case, the phase margin (\( \Phi_M \)) can be severely degraded, resulting in excessive ringing or even oscillation.

A simple way to overcome this problem is to insert a capacitor in the feedback path, as shown in Figure 60.

The resulting pole can be positioned to adjust the phase margin. Setting \( C_r = (R_1/R_2) C_t \) achieves a phase margin of 90°.

**REDUCING ELECTROMAGNETIC INTERFERENCE**

A number of methods can be utilized to reduce the effects of EMI on amplifier circuits.

In one method, stray signals on either input are coupled to the opposite input of the amplifier. The result is that the signal is rejected according to the CMRR of the amplifier. This is usually achieved by inserting a capacitor between the inputs of the amplifier, as shown in Figure 61. However, this method can also cause instability, depending on the value of capacitance.

Placing a resistor in series with the capacitor (see Figure 62) increases the dc loop gain and reduces the output error. Positioning the breakpoint (introduced by R-C) below the secondary pole of the operational amplifier improves the phase margin and, therefore, stability.

\[ R = \frac{R_2}{a(f_2)} - \left(1 + \frac{R_2}{R_1}\right) \]

where:

- \( a \) is the open-loop gain of the amplifier.
- \( f_2 \) is the frequency at which the phase of \( a = \Phi_M - 180° \).
PROPER BOARD LAYOUT
The OPx177 is a high precision device. To ensure optimum performance at the PCB level, care must be taken in the design of the board layout.

To avoid leakage currents, the surface of the board should be kept clean and free of moisture. Coating the surface creates a barrier to moisture accumulation and helps reduce parasitic resistance on the board.

Keeping supply traces short and properly bypassing the power supplies minimizes power supply disturbances due to output current variation, such as when driving an ac signal into a heavy load. Bypass capacitors should be connected as closely as possible to the device supply pins. Stray capacitances are a concern at the outputs and the inputs of the amplifier. It is recommended that signal traces be kept at least 5 mm from supply lines to minimize coupling.

A variation in temperature across the PCB can cause a mismatch in the Seebeck voltages at solder joints and other points where dissimilar metals are in contact, resulting in thermal voltage errors. To minimize these thermocouple effects, orient resistors so heat sources warm both ends equally. Input signal paths should contain matching numbers and types of components, where possible to match the number and type of thermocouple junctions. For example, dummy components such as zero value resistors can be used to match real resistors in the opposite input path. Matching components should be located in close proximity and should be oriented in the same manner. Ensure leads are of equal length so that thermal conduction is in equilibrium. Keep heat sources on the PCB as far away from amplifier input circuitry as is practical.

The use of a ground plane is highly recommended. A ground plane reduces EMI noise and also helps to maintain a constant temperature across the circuit board.

DIFFERENCE AMPLIFIERS
Difference amplifiers are used in high accuracy circuits to improve the common-mode rejection ratio (CMRR).

In the single instrumentation amplifier (see Figure 63), where

\[
\frac{R4}{R3} = \frac{R2}{R1}
\]

\[
V_o = \frac{R2}{R1} (V_2 - V_1)
\]

a mismatch between the ratio R2/R1 and R4/R3 causes the common-mode rejection ratio to be reduced.

To better understand this effect, consider that, by definition,

\[
CMRR = \frac{A_{DM}}{A_{CM}}
\]

where ADM is the differential gain and ACM is the common-mode gain.

\[
A_{DM} = \frac{V_o}{V_{DIFF}} \quad \text{and} \quad A_{CM} = \frac{V_o}{V_{CM}}
\]

\[
V_{DIFF} = V_i - V_2 \quad \text{and} \quad V_{CM} = \frac{1}{2}(V_i + V_2)
\]

For this circuit to act as a difference amplifier, its output must be proportional to the differential input signal.

From Figure 63,

\[
V_o = \left( \frac{R2}{R1} \right) V_i + \left[ \frac{1 + \frac{R2}{R1}}{1 + \frac{R3}{R4}} \right] V_2
\]

Arranging terms and combining the previous equations yields

\[
CMRR = \frac{R4R1 + R3R2 + 2R4R2}{2R4R1 - 2R2R3} \quad (1)
\]

The sensitivity of CMRR with respect to the R1 is obtained by taking the derivative of CMRR, in Equation 1, with respect to R1.

\[
\frac{\delta CMRR}{\delta R1} = \frac{\delta}{\delta R1} \left( \frac{R1R4}{2R1R4 - 2R2R3} + \frac{2R2R4 + R2R3}{2R1R4 - 2R2R3} \right)
\]

\[
\frac{\delta CMRR}{\delta R1} = \frac{1}{2} \left( \frac{1}{2R2R3} \right) \frac{R1R4}{R1R4}
\]

Assuming that

\[
R1 \approx R2 \approx R3 \approx R4 \approx R
\]

and

\[
R(1 - \delta) < R1, R2, R3, R4 < R(1 + \delta)
\]

the worst-case CMRR error arises when

\[
R1 = R4 = R(1 + \delta) \quad \text{and} \quad R2 = R3 = R(1 - \delta)
\]
Plugging these values into Equation 1 yields

\[ \text{CMRR}_{\text{MIN}} \approx \frac{1}{20} \]

where \( \delta \) is the tolerance of the resistors.

Lower tolerance value resistors result in higher common-mode rejection (up to the CMRR of the operational amplifier).

Using 5% tolerance resistors, the highest CMRR that can be guaranteed is 20 dB. Alternatively, using 0.1% tolerance resistors results in a common-mode rejection ratio of at least 54 dB (assuming that the operational amplifier CMRR \( \times 54 \) dB).

With the CMRR of OPx177 at 120 dB minimum, the resistor match is the limiting factor in most circuits. A trimming resistor can be used to further improve resistor matching and CMRR of the difference amplifier circuit.

**A HIGH ACCURACY THERMOCOUPLE AMPLIFIER**

A thermocouple consists of two dissimilar metal wires placed in contact. The dissimilar metals produce a voltage

\[ V_{TC} = \alpha (T_J - T_R) \]

where:

- \( T_J \) is the temperature at the measurement of the hot junction.
- \( T_R \) is the temperature at the cold junction.
- \( \alpha \) is the Seebeck coefficient specific to the dissimilar metals used in the thermocouple.
- \( V_{TC} \) is the thermocouple voltage and becomes larger with increasing temperature.

Maximum measurement accuracy requires cold junction compensation of the thermocouple. To perform the cold junction compensation, apply a copper wire short across the terminating junctions (inside the isothermal block) simulating a 0°C point. Adjust the output voltage to zero using the R5 trimming resistor, and remove the copper wire.

The OPx177 is an ideal amplifier for thermocouple circuits because it has a very low offset voltage, excellent PSRR and CMRR, and low noise at low frequencies.

It can be used to create a thermocouple circuit with great linearity. Resistor R1, Resistor R2, and Diode D1, shown in Figure 64, are mounted in an isothermal block.

**LOW POWER LINEARIZED RTD**

A common application for a single element varying bridge is an RTD thermometer amplifier, as shown in Figure 65. The excitation is delivered to the bridge by a 2.5 V reference applied at the top of the bridge.

RTDs may have thermal resistance as high as 0.5°C to 0.8°C per mW. To minimize errors due to resistor drift, the current through each leg of the bridge must be kept low. In this circuit, the amplifier supply current flows through the bridge. However, at the OPx177 maximum supply current of 600 µA, the RTD dissipates less than 0.1 mW of power, even at the highest resistance. Errors due to power dissipation in the bridge are kept under 0.1°C.

Calibration of the bridge is made at the minimum value of temperature to be measured by adjusting \( R_P \) until the output is zero. To calibrate the output span, set the full-scale and linearity potentiometers to midpoint and apply a 500°C temperature to the sensor or substitute the equivalent 500°C RTD resistance. Adjust the full-scale potentiometer for a 5 V output. Finally, apply 250°C or the equivalent RTD resistance and adjust the linearity potentiometer for 2.5 V output. The circuit achieves better than ±0.5°C accuracy after adjustment.
SINGLE OPERATIONAL AMPLIFIER BRIDGE

The low input offset voltage drift of the OP1177 makes it very effective for bridge amplifier circuits used in RTD signal conditioning. It is often more economical to use a single bridge operational amplifier as opposed to an instrumentation amplifier.

In the circuit shown in Figure 66, the output voltage at the operational amplifier is

\[
V_O = \frac{R_2}{R} V_{REF} \left[ \frac{\delta}{1 + \frac{R_1}{R} + \frac{R_1}{R_2} (1 + \delta)} \right]
\]

where \( \delta = \Delta R/R \) is the fractional deviation of the RTD resistance with respect to the bridge resistance due to the change in temperature at the RTD.

For \( \delta << 1 \), the preceding expression becomes

\[
V_O \approx \left( \frac{R_2}{R} \right) V_{REF} \left[ \frac{\delta}{1 + \frac{R_1}{R} + \frac{R_1}{R_2}} \right] \]

With \( V_{REF} \) constant, the output voltage is linearly proportional to \( \delta \) with a gain factor of

\[
V_{REF} \left[ \frac{R_2}{R} \right] \left[ 1 + \frac{R_1}{R_2} \right]
\]
REALIZATION OF ACTIVE FILTERS

BAND-PASS KRC OR SALLEN-KEY FILTER

The low offset voltage and the high CMRR of the OPx177 make it an excellent choice for precision filters, such as the band-pass KRC filter shown in Figure 67. This filter type offers the capability to tune the gain and the cutoff frequency independently.

Because the common-mode voltage into the amplifier varies with the input signal in the KRC filter circuit, a high CMRR is required to minimize distortion. Also, the low offset voltage of the OPx177 allows a wider dynamic range when the circuit gain is chosen to be high.

The circuit of Figure 67 consists of two stages. The first stage is a simple high-pass filter where the corner frequency \( f_c \) is

\[
\frac{1}{2\pi \sqrt{C_1 C_2 R_1 R_2}} \tag{2}
\]

and

\[ Q = K \frac{R_1}{R_2} \tag{3} \]

where \( K \) is the dc gain.

Choosing equal capacitor values minimizes the sensitivity and simplifies Equation 2 to

\[
\frac{1}{2\pi \sqrt{R_1 R_2}} \tag{2}
\]

The value of \( Q \) determines the peaking of the gain vs. frequency (ringing in transient response). Commonly chosen values for \( Q \) are generally near unity.

Setting \( Q = \frac{1}{\sqrt{2}} \) yields minimum gain peaking and minimum ringing. Determine values for \( R_1 \) and \( R_2 \) by using Equation 3.

For \( Q = \frac{1}{\sqrt{2}} \), \( R_1/R_2 = 2 \) in the circuit example. Select \( R_1 = 5 \, \text{k}\Omega \) and \( R_2 = 10 \, \text{k}\Omega \) for simplicity.

The second stage is a low-pass filter where the corner frequency can be determined in a similar fashion. For \( R_3 = R_4 = R \)

\[
f_c = \frac{1}{2\pi R \sqrt{C_3}} \quad \text{and} \quad Q = \frac{1}{2} \sqrt{C_3 \over C_4}
\]

CHANNEL SEPARATION

Multiple amplifiers on a single die are often required to reject any signals originating from the inputs or outputs of adjacent channels. OP2177 input and bias circuitry is designed to prevent feedthrough of signals from one amplifier channel to the other. As a result, the OP2177 has an impressive channel separation of greater than \(-120 \, \text{dB} \) for frequencies up to \(100 \, \text{kHz} \) and greater than \(-115 \, \text{dB} \) for signals up to 1 MHz.

REFERENCES ON NOISE DYNAMICS AND FLICKER NOISE


OUTLINE DIMENSIONS

COMPLIANT TO JEDEC STANDARDS MS-012-AA
CONTROLLING DIMENSIONS ARE IN MILLIMETERS; INCH DIMENSIONS (IN PARENTHESES) ARE ROUNDED-OFF MILLIMETER EQUIVALENTS FOR REFERENCE ONLY AND ARE NOT APPROPRIATE FOR USE IN DESIGN.

Figure 69. 8-Lead Standard Small Outline Package [SOIC_N] Narrow Body (R-8)
Dimensions shown in millimeters and (inches)

COMPLIANT TO JEDEC STANDARDS MS-012-AB
CONTROLLING DIMENSIONS ARE IN MILLIMETERS; INCH DIMENSIONS (IN PARENTHESES) ARE ROUNDED-OFF MILLIMETER EQUIVALENTS FOR REFERENCE ONLY AND ARE NOT APPROPRIATE FOR USE IN DESIGN.

Figure 70. 14-Lead Standard Small Outline Package [SOIC_N] Narrow Body (R-14)
Dimensions shown in millimeters and (inches)
Figure 71. 8-Lead Mini Small Outline Package (MSOP) (RM-8)
Dimensions shown in millimeters

Figure 72. 14-Lead Thin Shrink Small Outline Package (TSSOP) (RU-14)
Dimensions shown in millimeters
## ORDERING GUIDE

<table>
<thead>
<tr>
<th>Model</th>
<th>Temperature Range</th>
<th>Package Description</th>
<th>Package Option</th>
<th>Marking Code</th>
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<tbody>
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<td>OP1177ARZ</td>
<td>−40°C to +125°C</td>
<td>8-Lead SOIC_N</td>
<td>R-8</td>
<td>AZA</td>
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<td>OP1177ARZ-REEL</td>
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<td>8-Lead SOIC_N</td>
<td>R-8</td>
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<tr>
<td>OP1177ARZ-REEL7</td>
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<td>8-Lead SOIC_N</td>
<td>R-8</td>
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</tr>
<tr>
<td>OP1177ARM-REEL</td>
<td>−40°C to +125°C</td>
<td>8-Lead MSOP</td>
<td>RM-8</td>
<td>AZA</td>
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<tr>
<td>OP1177ARMZ</td>
<td>−40°C to +125°C</td>
<td>8-Lead MSOP</td>
<td>RM-8</td>
<td>AZA</td>
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<td>OP1177ARMZ-REEL</td>
<td>−40°C to +125°C</td>
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<td>OP1177ARMZ-R7</td>
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<td>8-Lead MSOP</td>
<td>RM-8</td>
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<td>8-Lead SOIC_N</td>
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<td>OP2177CRZ-REEL7</td>
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1 Z = RoHS Compliant Part.