FEATURES

- Uses Tiny Capacitors and Inductor
- Internally Compensated
- Fixed Frequency 1.4MHz Operation
- Operates with \( V_{IN} \) as Low as 1.1V
- 3V at 30mA from a Single Cell
- 5V at 200mA from 3.3V Input
- 15V at 60mA from Four Alkaline Cells
- High Output Voltage: Up to 34V
- Low Shutdown Current: <1\( \mu \)A
- Low \( V_{CESAT} \) Switch: 300mV at 300mA
- Tiny 5-Lead SOT-23 Package

APPLICATIONS

- Digital Cameras
- Pagers
- Cordless Phones
- Battery Backup
- LCD Bias
- Medical Diagnostic Equipment
- Local 5V or 12V Supply
- External Modems
- PC Cards

DESCRIPTION

The LT\textsuperscript{®}1613 is the industry’s first 5-lead SOT-23 current
mode DC/DC converter. Intended for small, low power
applications, it operates from an input voltage as low as
1.1V and switches at 1.4MHz, allowing the use of tiny, low
cost capacitors and inductors 2mm or less in height. Its
small size and high switching frequency enables the
complete DC/DC converter function to take up less than
0.2 square inches of PC board area. Multiple output power
supplies can now use a separate regulator for each output
voltage, replacing cumbersome quasi-regulated ap-
proaches using a single regulator and a custom trans-
former.

A constant frequency, internally compensated current
mode PWM architecture results in low, predictable output
noise that is easy to filter. The high voltage switch on the
LT1613 is rated at 36V, making the device ideal for boost
converters up to 34V as well as for Single-Ended Primary
Inductance Converter (SEPIC) and flyback designs. The
device can generate 5V at up to 200mA from a 3.3V supply
or 5V at 175mA from four alkaline cells in a SEPIC design.

The LT1613 is available in the 5-lead SOT-23 package.

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TYPICAL APPLICATION

Figure 1. 3.3V to 5V 200mA DC/DC Converter

![Efficiency Curve](image-url)
### ELECTRICAL CHARACTERISTICS

The \( \bullet \) denotes the specifications which apply over the full operating temperature range, otherwise specifications are at \( T_A = 25^\circ C \). Commercial grade \( 0^\circ C \) to \( 70^\circ C \), \( V_{IN} = 1.5V \), \( V_{SHDN} = V_{IN} \) unless otherwise noted. (Note 2)

<table>
<thead>
<tr>
<th>PARAMETER</th>
<th>CONDITIONS</th>
<th>MIN</th>
<th>TYP</th>
<th>MAX</th>
<th>UNITS</th>
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<tr>
<td>Minimum Operating Voltage</td>
<td></td>
<td>0.9</td>
<td>1.1</td>
<td></td>
<td>V</td>
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<tr>
<td>Maximum Operating Voltage</td>
<td></td>
<td>10</td>
<td></td>
<td></td>
<td>V</td>
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<tr>
<td>Feedback Voltage</td>
<td>( \bullet )</td>
<td>1.205</td>
<td>1.23</td>
<td>1.255</td>
<td>V</td>
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<tr>
<td>FB Pin Bias Current</td>
<td>( \bullet )</td>
<td>27</td>
<td>80</td>
<td></td>
<td>mA</td>
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<td>Quiescent Current</td>
<td>( V_{SHDN} = 1.5V )</td>
<td>3</td>
<td>4.5</td>
<td></td>
<td>mA</td>
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<tr>
<td>Quiescent Current in Shutdown</td>
<td>( V_{SHDN} = 0V, V_{IN} = 2V )</td>
<td>0.01</td>
<td>0.5</td>
<td></td>
<td>( \mu )A</td>
</tr>
<tr>
<td></td>
<td>( V_{SHDN} = 0V, V_{IN} = 5V )</td>
<td>0.01</td>
<td>1.0</td>
<td></td>
<td>( \mu )A</td>
</tr>
<tr>
<td>Reference Line Regulation</td>
<td>( 1.5V \leq V_{IN} \leq 10V )</td>
<td>0.02</td>
<td>0.2</td>
<td></td>
<td>%/V</td>
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<tr>
<td>Switching Frequency</td>
<td>( \bullet )</td>
<td>1.0</td>
<td>1.4</td>
<td>1.8</td>
<td>MHz</td>
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<td>Maximum Duty Cycle</td>
<td>( \bullet )</td>
<td>82</td>
<td>86</td>
<td></td>
<td>%</td>
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<td>Switch Current Limit</td>
<td>(Note 3)</td>
<td>550</td>
<td>800</td>
<td></td>
<td>mA</td>
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<tr>
<td>Switch ( V_{CESAT} )</td>
<td>( I_{SW} = 300mA )</td>
<td>300</td>
<td>350</td>
<td></td>
<td>mV</td>
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<td>Switch Leakage Current</td>
<td>( V_{SW} = 5V )</td>
<td>0.01</td>
<td>1</td>
<td></td>
<td>\muA</td>
</tr>
<tr>
<td>SHDN Input Voltage High</td>
<td></td>
<td>1</td>
<td></td>
<td></td>
<td>V</td>
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<tr>
<td>SHDN Input Voltage Low</td>
<td></td>
<td>0.3</td>
<td></td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>SHDN Pin Bias Current</td>
<td>( V_{SHDN} = 3V )</td>
<td>25</td>
<td>50</td>
<td></td>
<td>\muA</td>
</tr>
<tr>
<td></td>
<td>( V_{SHDN} = 0V )</td>
<td>0.01</td>
<td>0.1</td>
<td></td>
<td>\muA</td>
</tr>
</tbody>
</table>

**Note 1:** Absolute Maximum Ratings are those values beyond which the life of a device may be impaired.

**Note 2:** The LT1613C is guaranteed to meet performance specifications from \( 0^\circ C \) to \( 70^\circ C \). Specifications over the \( -40^\circ C \) to \( 85^\circ C \) operating temperature range are assured by design, characterization and correlation with statistical process controls.

**Note 3:** Current limit guaranteed by design and/or correlation to static test.
TYPICAL PERFORMANCE CHARACTERISTICS

Switch $V_{CESAT}$ vs Switch Current

Oscillator Frequency vs Temperature

SHDN Pin Current vs $V_{SRDN}$

Current Limit vs Duty Cycle

Feedback Pin Voltage

Switching Waveforms, Circuit of Figure 1
**PIN FUNCTIONS**

**SW (Pin 1):** Switch Pin. Connect inductor/diode here. Minimize trace area at this pin to keep EMI down.

**GND (Pin 2):** Ground. Tie directly to local ground plane.

**FB (Pin 3):** Feedback Pin. Reference voltage is 1.23V. Connect resistive divider tap here. Minimize trace area at FB. Set \( V_{OUT} \) according to \( V_{OUT} = 1.23V(1 + R1/R2) \).

**SHDN (Pin 4):** Shutdown Pin. Tie to 1V or more to enable device. Ground to shut down.

**V\text{IN} (Pin 5):** Input Supply Pin. Must be locally bypassed.

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**BLOCK DIAGRAM**

![Block Diagram of LT1613](image)

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**OPERATION**

The LT1613 is a current mode, internally compensated, fixed frequency step-up switching regulator. Operation can be best understood by referring to the Block Diagram. Q1 and Q2 form a bandgap reference core whose loop is closed around the output of the regulator. The voltage drop across R5 and R6 is low enough such that Q1 and Q2 do not saturate, even when \( V_{IN} \) is 1V. When there is no load, FB rises slightly above 1.23V, causing \( V_C \) (the error amplifier’s output) to decrease. Comparator A2’s output stays high, keeping switch Q3 in the off state. As increased output loading causes the FB voltage to decrease, A1’s output increases. Switch current is regulated directly on a cycle-by-cycle basis by the \( V_C \) node. The flip flop is set at the beginning of each switch cycle, turning on the switch. When the summation of a signal representing switch current and a ramp generator (introduced to avoid subharmonic oscillations at duty factors greater than 50%) exceeds the \( V_C \) signal, comparator A2 changes state, resetting the flip flop and turning off the switch. More power is delivered to the output as switch current is increased. The output voltage, attenuated by external resistor divider R1 and R2, appears at the FB pin, closing the overall loop. Frequency compensation is provided internally by \( R_C \) and \( C_C \). Transient response can be optimized by the addition of a phase lead capacitor \( C_{PL} \) in parallel with \( R_1 \) in applications where large value or low ESR output capacitors are used.

As the load current is decreased, the switch turns on for a shorter period each cycle. If the load current is further decreased, the converter will skip cycles to maintain output voltage regulation.
OPERATION

LAYOUT

The LT1613 switches current at high speed, mandating careful attention to layout for proper performance. You will not get advertised performance with careless layouts. Figure 2 shows recommended component placement for a boost (step-up) converter. Follow this closely in your PCB layout. Note the direct path of the switching loops. Input capacitor C1 must be placed close (<5mm) to the IC package. As little as 10mm of wire or PC trace from Cin to Vin will cause problems such as inability to regulate or oscillation.

The ground terminal of output capacitor C2 should tie close to Pin 2 of the LT1613. Doing this reduces dI/dt in the ground copper which keeps high frequency spikes to a minimum. The DC/DC converter ground should tie to the PC board ground plane at one place only, to avoid introducing dI/dt in the ground plane.

A SEPIC (single-ended primary inductance converter) schematic is shown in Figure 3. This converter topology produces a regulated output voltage that spans (i.e., can be higher or lower than) the output. Recommended component placement for a SEPIC is shown in Figure 4.

COMPONENT SELECTION

Inductors

Inductors used with the LT1613 should have a saturation current rating (where inductance is approximately 70% of zero current inductance) of approximately 0.5A or greater. DCR of the inductors should be 0.5Ω or less. For boost converters, inductance should be 4.7mH for input voltage less than 3.3V and 10mH for inputs above 3.3V. When using the device as a SEPIC, either a coupled inductor or two separate inductors can be used. If using separate inductors, 22mH units are recommended for input voltage above 3.3V. Coupled inductors have a beneficial mutual inductance, so a 10mH coupled inductor results in the same ripple current as two 20mH uncoupled units.
**OPERATION**

Table 1 lists several inductors that will work with the LT1613, although this is not an exhaustive list. There are many magnetics vendors whose components are suitable for use.

**Diodes**

A Schottky diode is recommended for use with the LT1613. The Motorola MBR0520 is a very good choice. Where the input to output voltage differential exceeds 20V, use the MBR0530 (a 30V diode). If cost is more important than efficiency, the 1N4148 can be used, but only at low current loads.

**Capacitors**

The input bypass capacitor must be placed physically close to the input pin. ESR is not critical and in most cases an inexpensive tantalum is appropriate.

The choice of output capacitor is far more important. The quality of this capacitor is the greatest determinant of the output voltage ripple. The output capacitor must have enough capacitance to satisfy the load under transient conditions and it must shunt the switched component of current coming through the diode. Output voltage ripple results when this switched current passes through the finite output impedance of the output capacitor. The capacitor should have low impedance at the 1.4MHz switching frequency of the LT1613. At this frequency, the impedance is usually dominated by the capacitor’s equivalent series resistance (ESR). Choosing a capacitor with lower ESR will result in lower output ripple.

Ceramic capacitors can be used with the LT1613 provided loop stability is considered. A tantalum capacitor has some ESR and this causes an “ESR zero” in the regulator loop. This zero is beneficial to loop stability. The internally compensated LT1613 does not have an accessible compensation node, but other circuit techniques can be employed to counteract the loss of the ESR zero, as detailed in the next section.

Some capacitor types appropriate for use with the LT1613 are listed in Table 2.

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**Table 1. Inductor Vendors**

<table>
<thead>
<tr>
<th>VENDOR</th>
<th>PHONE</th>
<th>URL</th>
<th>PART</th>
<th>COMMENT</th>
</tr>
</thead>
<tbody>
<tr>
<td>Sumida</td>
<td>(847) 956-0666</td>
<td><a href="http://www.sumida.com">www.sumida.com</a></td>
<td>CLS62-22022, CD43-220</td>
<td>22μH Coupled 22μH</td>
</tr>
<tr>
<td>Murata</td>
<td>(404) 436-1300</td>
<td><a href="http://www.murata.com">www.murata.com</a></td>
<td>LQH3C-220, LQH3C-100, LQH3C-4R7</td>
<td>22μH, 2mm Height 10μH, 4.7μH</td>
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<tr>
<td>Coiltronics</td>
<td>(407) 241-7876</td>
<td><a href="http://www.coiltronics.com">www.coiltronics.com</a></td>
<td>CTX20-1</td>
<td>20μH Coupled, Low DCR</td>
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**Table 2. Capacitor Vendors**

<table>
<thead>
<tr>
<th>VENDOR</th>
<th>PHONE</th>
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<th>COMMENT</th>
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<tbody>
<tr>
<td>Taiyo Yuden</td>
<td>(408) 573-4150</td>
<td><a href="http://www.t-yuden.com">www.t-yuden.com</a></td>
<td>Ceramic Caps</td>
<td>X5R Dielectric</td>
</tr>
<tr>
<td>AVX</td>
<td>(803) 448-9411</td>
<td><a href="http://www.avxcorp.com">www.avxcorp.com</a></td>
<td>Ceramic Caps, Tantalum Caps</td>
<td></td>
</tr>
<tr>
<td>Murata</td>
<td>(404) 436-1300</td>
<td><a href="http://www.murata.com">www.murata.com</a></td>
<td>Ceramic Caps</td>
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</tr>
</tbody>
</table>

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resulting in a severely underdamped response. By adding R3 and C\textsubscript{PL} as detailed in Figure 8’s schematic, phase margin is restored, and transient response to the same load step is pictured in Figure 9. R3 isolates the device FB pin from fast edges on the V\textsubscript{OUT} node due to parasitic PC trace inductance.

Figure 10’s circuit details a 5V to 12V boost converter, delivering up to 130mA. The transient response to a load step of 10mA to 130mA, without C\textsubscript{PL}, is pictured in Figure 11. Although the ringing is less than that of the previous example, the response is still underdamped and can be improved. After adding R3 and C\textsubscript{PL}, the improved transient response is detailed in Figure 12.

Figure 13 shows a SEPIC design, converting a 3V to 10V input to a 5V output. The transient response to a load step of 20mA to 120mA, without C\textsubscript{PL} and R3, is pictured in Figure 14. After adding these two components, the improved response is shown in Figure 15.
**LT1613**

**OPERATION**

![LT1613 Circuit Diagram]

**Figure 10. 5V to 12V Boost Converter with 4.7μF Ceramic Output Capacitor, CPL Added to Increase Phase Margin**

- **Vin**: 5V
- **Vout**: 12V
- **Load Current**: 130mA
- **C1**: AVX TAJB226M010
- **C2**: TAIYO YUDEN EMK325BJ475MN
- **D1**: MOTOROLA MBR0520
- **L1**: MURATA LQH3C100

![Waveform 1](image)

**Figure 11. 5V to 12V Boost Converter with 4.7μF Ceramic Output Capacitor**

- **Vin**: 5V
- **Vout**: 12V
- **Load Current**: 130mA

![Waveform 2](image)

**Figure 12. 5V to 12V Boost Converter with 4.7μF Ceramic Output Capacitor and 200pF Phase-Lead Capacitor CPL and 10k in Series with FB Pin**

- **Vin**: 3V TO 10V
- **Vout**: 12V
- **Load Current**: 120mA

![Waveform 3](image)

**Figure 13. 5V Output SEPIC with Ceramic Output Capacitor, CPL Adds Phase Margin**

- **Vin**: 3V TO 10V
- **Vout**: 5V
- **Load Current**: 20mA

![Waveform 4](image)

**Figure 14. 5V Output SEPIC with 10μF Ceramic Output Capacitor. No CPL. Vin = 4V**

- **Vout**: 50mV/DIV
- **Load Current**: 120mA

![Waveform 5](image)

**Figure 15. 5V Output SEPIC with 10μF Ceramic Output Capacitor, 330pF CPL and 10k in Series with FB Pin**

- **Vout**: 50mV/DIV
- **Load Current**: 20mA
START-UP/SOFT-START

When the LT1613 SHDN pin voltage goes high, the device rapidly increases the switch current until internal current limit is reached. Input current stays at this level until the output capacitor is charged to final output voltage. Switch current can exceed 1A. Figure 16's oscillograph details start-up waveforms of Figure 17’s SEPIC into a 50Ω load without any soft-start. The output voltage reaches final value in approximately 200μs, while input current reaches 400mA. Switch current in a SEPIC is 2x the input current, so the switch is conducting approximately 800mA peak.

Soft-start reduces the inrush current by taking more time to reach final output voltage. A soft-start circuit consisting of Q1, R_S1, R_S2 and C_S as shown in Figure 17 can be used to limit inrush current to a lower value. Figure 18 pictures V_OUT and input current with R_S2 of 33kΩ and C_S of 10nF. Input current is limited to a peak value of 200mA as the time required to reach final value increases to 1.7ms. In Figure 19, C_S is increased to 33nF. Input current does not exceed the steady-state current the device uses to supply power to the 50Ω load. Start-up time increases to 4.3ms. C_S can be increased further for an even slower ramp, if desired.
TYPICAL APPLICATIONS

4-Cell to 5V SEPIC DC/DC Converter

4-Cell to 15V/30mA DC/DC Converter

3.3V to 8V/70mA, –8V/5mA, 24V/5mA TFT LCD Bias Supply Uses All Ceramic Capacitors
4-Cell to 5V/50mA, 12V/10mA, 15V/10mA Digital Camera Power Supply

C1: TAIYO YUDEN JMK316BJ106ML
C2, C3, C4: TAIYO YUDEN EMK212BJ105MG
C5: TAIYO YUDEN JMK212BJ475MG
D1: MOTOROLA MBR0520
D2, D3: BAT54
T1: COILCRAFT CCI8245A       (847) 639-6400

VIN 7V TO 3.6V

15V/10mA

12V/10mA

5V/50mA

–7.5V/10mA

C1 10µF
C2 1µF
C3 1µF
C4 1µF
C5 4.7µF

270pF

33.2k

102k

4-Cell to 5V/50mA, 15V/10mA, –7.5V/10mA Digital Camera Power Supply

C1: TAIYO YUDEN JMK316BJ106ML
C2, C3, C4: TAIYO YUDEN EMK212BJ105MG
C5: TAIYO YUDEN JMK212BJ475MG
D1: MOTOROLA MBR0520
D2, D3: BAT54
T1: COILCRAFT CCI8244A       (847) 639-6400

VIN 7V TO 3.6V

15V/10mA

5V/50mA

–7.5V/10mA

C1 10µF
C2 1µF
C3 1µF
C4 1µF
C5 4.7µF

270pF

33.2k

102k

Information furnished by Linear Technology Corporation is believed to be accurate and reliable. However, no responsibility is assumed for its use. Linear Technology Corporation makes no representation that the interconnection of its circuits as described hereon will not infringe on existing patent rights.
**TYPICAL APPLICATIONS**

Li-ion to 16V/20mA Step-Up DC/DC Converter

![Circuit Diagram]

**PACKAGE DESCRIPTION**

Dimensions in inches (millimeters) unless otherwise noted.

**S5 Package**

5-Lead Plastic SOT-23

(LTC DWG # 05-08-1633)

**RELATED PARTS**

<table>
<thead>
<tr>
<th>PART NUMBER</th>
<th>DESCRIPTION</th>
<th>COMMENTS</th>
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<td>Single Cell Micropower DC/DC</td>
<td>3.3V/75mA From 1V; 600kHz Fixed Frequency</td>
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<tr>
<td>LT1317</td>
<td>2-Cell Micropower DC/DC</td>
<td>3.3V/200mA From Two Cells; 600kHz Fixed Frequency</td>
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<td>LTC1474</td>
<td>Low Quiescent Current, High Efficiency Step-Down Converter</td>
<td>94% Efficiency, 10μA I(_Q), 9V to 5V at 250μA</td>
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<td>LT1521</td>
<td>300mA Low Dropout Regulator with Micropower Quiescent Current and Shutdown</td>
<td>500mV Dropout, 300mA Output Current, 12μA I(_Q)</td>
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<tr>
<td>LTC1517-5</td>
<td>Micropower, Regulated Charge Pump</td>
<td>3-Cells to 5V at 20mA, SOT-23 Package, 6μA I(_Q)</td>
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<td>LT1610</td>
<td>1.7MHz Single Cell Micropower DC/DC Converter</td>
<td>30μA I(_Q), MSOP Package, Internal Compensation</td>
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<tr>
<td>LT1611</td>
<td>Inverting 1.4MHz Switching Regulator</td>
<td>5V to –5V at 150mA, Low Output Noise</td>
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<td>Micropower DC/DC Converter in 5-Lead SOT-23</td>
<td>20V at 12mA from 2.5V Input, Tiny SOT-23 Package</td>
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